

AI - IoT Integrated Railway Safety Framework for Real - Time Collision Mitigation and Animal Intrusion Detection

Dr.S.Saravanan, Mrs.S.Rajeswari, Deepadharsanan S, Devendhiran V, Hariharan S, Kamesh G

Department of Electrical and Electronics Engineering, Muthayammal Engineering College, (Autonomous), Rasipuram, Tamil Nadu, India

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ABSTRACT: Recent and next-generation wireless broadcasting standards, such as DVB-T2 or DVB-NGH, are considering distributed multi-antenna transmission in order to increase bandwidth efficiency and signal quality. The main goal is to combine diversity and spatial multiplexing in order to fully exploit the channel capacity. Full-rate full-diversity (FRFD) space-time codes (STC), such as the Golden code, have been reported to be excellent candidates, being their main drawback their detection complexity, which is enhanced when soft output is required when combined with a bit interleaved coded modulation (BICM) scheme based on low-density parity check (LDPC) codes. We present a novel low-complexity soft detection algorithm for the reception of Golden codes in LDPC based orthogonal frequency-division multiplexing (OFDM) systems. Complexity and simulation-based performance results are provided which show that the proposed detector performs close to the optimal detector in a variety of DVB-T2 broadcasting scenarios.

KEYWORDS: MAP detection, Space-Frequency Block Coding (SFBC), Low-density parity check (LDPC) codes, Orthogonal Frequency Division Multiplexing (OFDM).

I. INTRODUCTION

The second generation of the terrestrial digital video broadcasting standard (DVB-T2) [1] has adopted a space-frequency block code (SFBC) based on the well-known Alamouti technique. In order to increase the capacity and reach the full multiple-input multiple-output (MIMO) diversity-multiplexing frontier, the proposals for the future generations of terrestrial, portable and mobile digital video broadcasting standards, such as DVB-NGH, focus on the combination of both diversity and spatial multiplexing [2, 3] through full-rate full diversity (FRFD) codes such as the Golden code. The main disadvantage of Golden codes arises from their very high decoding complexity, which is enhanced when iterative decoders, such as turbo or low-density parity check (LDPC) codes, are included in the reception chain, since soft information on the conditional probabilities for all possible transmitted symbols is required in the form of log-likelihood

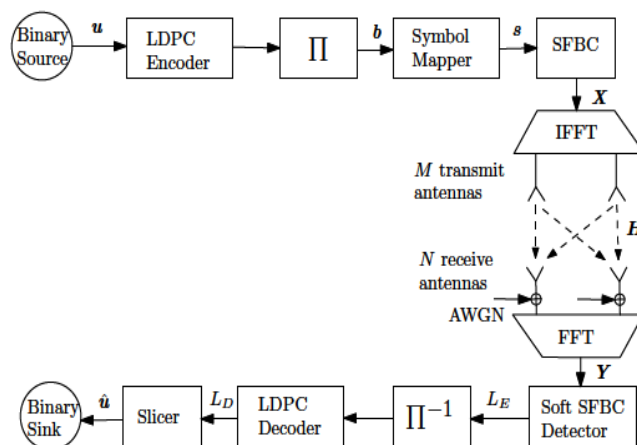


Figure 1 .Simplified diagram of a LDPC-based SFBC OFDM transmission and reception scheme based on DVB-T2.



ratios (LLR), which is unfeasible for high constellation sizes.

This paper presents the design of a low-complexity soft detection algorithm for Golden codes in bit-interleaved coded modulation (BICM) OFDM systems based on LDPC coding. The generation of the candidate list is carried out by means of a fixed tree search, whose complexity does not depend on the channel conditions or the noise level. Since the complexity of the proposed soft detector is closely linked to the architecture of the tree search, we analyze different tree configurations in

Order to find the best balance between complexity and performance. Simulation results are provided for the Golden [14] code in a DVB-T2 framework [15]. Although this has been carried out on a terrestrial TV system.

The contribution of this paper is a new low-complexity soft detection algorithm for FRFD SFBC and its assessment in an LDPC-based BICM scenario. The generation of the candidate list is carried out by means of a fixed tree search, whose complexity does not depend on the channel conditions or the noise level. Since the complexity of the proposed soft detector is closely linked to the architecture of the tree search, we analyze different tree configurations in order to find the best balance between complexity and performance. Simulation results are provided for the Golden [14] and the FRFD Sezginer-Sari (SS) codes [8] in a DVB-T2 framework [15]. Although our research has been carried out on a terrestrial TV system, the results can be generalized for any MIMO bit interleaved coded modulation (MIMO-BICM) scheme.

In section II, we present the system model. In section III, we present the Fixed Complexity Detection. In section IV, we present the simulation results are discussed. Section VI concludes the paper.

II. SYSTEM MODEL

Fig. 1 shows the considered LDPC-coded OFDM scheme with two transmit ($M = 2$) and two receive ($N = 2$) antennas. As can be seen, the bit stream is coded, interleaved and mapped onto a complex constellation. Next, a vector of Q symbols \mathbf{S} is coded into space and frequency forming the code word \mathbf{X} , which is transformed into the time domain by an inverse fast Fourier transform (IFFT) block and transmitted after the addition of a cyclic prefix. At the receiver side, the prefix is removed, a fast Fourier transform (FFT) is carried out and the resulting signal \mathbf{Y} of dimensions $N \times T$ can be represented mathematically as

$$\mathbf{Y} = \mathbf{H}\mathbf{X} + \mathbf{Z} \quad (1)$$

Where \mathbf{H} denotes the $N \times M$ complex channel matrix, \mathbf{X} is any $M \times T$ codeword matrix composed by a linear combination of Q data symbols and \mathbf{Z} represents the $N \times T$ zero-mean additive white Gaussian noise (AWGN) matrix whose complex coefficients fulfill $\mathcal{CN}(0, 2\sigma)$, being σ^2 the noise variance per real component. The design of the codeword \mathbf{X} follows the criteria defined in [16], [17] and will provide full rate when $Q = MT$, being T the frequency depth of the codeword. By taking the elements column-wise from matrices \mathbf{X} , \mathbf{Y} and \mathbf{Z} , equation (1) can be vectorized as

$$\mathbf{y} = \tilde{\mathbf{H}}\mathbf{G}\mathbf{s} + \mathbf{z} \quad (2)$$

where \mathbf{y} , \mathbf{s} and \mathbf{z} are column vectors. The matrix $\tilde{\mathbf{H}}$ is the equivalent $NT \times MT$ MIMO channel written as

$$\tilde{\mathbf{H}} = \begin{bmatrix} \mathbf{H}_1 & \dots & \mathbf{0} \\ \vdots & \ddots & \vdots \\ \mathbf{0} & \dots & \mathbf{H}_T \end{bmatrix} \quad (3)$$

where we have a block diagonal of channel realizations \mathbf{H}_c at the carriers $c = 1, \dots, T$. The complex coefficient h_{cij} corresponds to the channel from transmit antenna j to receive antenna i at the c -th carrier. The off-diagonal entries are zero matrices with dimensions $N \times M$. The matrix \mathbf{G} is the generator matrix for the SFBC such that $\mathbf{X} = \mathbf{G}\mathbf{s}$, where \mathbf{s} corresponds to the symbol column vector $[\mathbf{s}_1, \dots, \mathbf{s}_Q]^T$.

III. FIXED-COMPLEXITY DETECTION

The design of efficient detection algorithms is one of the greatest challenges when implementing full-rate SFBC. Given the high complexity of performing an exhaustive search, special focus has been drawn into developing lower complexity detection algorithms that yield a close-to-ML performance. The LSD is one of the most remarkable approach but its complexity order is bounded by $O(PQ)$ in the same way as the SD [9]. Even though the list of candidates corresponds to the set L of the smallest metrics, the complexity of performing such a selection may be considerably high for low signal-to noise ratio (SNR) scenarios. Furthermore, an unsuitable choice of the initial radius may lead to a shortage in candidate points, which forces the algorithm to restart with a looser sphere Constraint.

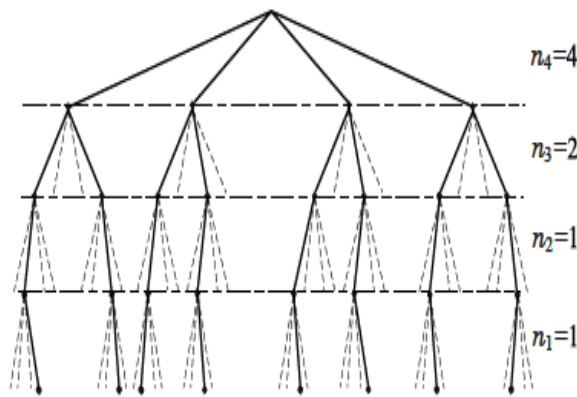


Figure2. Fixed-complexity tree search of a QPSK-modulated signal using a tree configuration vector of $n = [1, 1, 2, 4]$.

In order to limit the complexity and to facilitate the computation of soft detected symbols, a fixed-complexity tree-search style algorithm was proposed in [18] for spatial multiplexing schemes, coined list fixed-complexity sphere decoder (LFSD). The main feature of the LFSD is that, instead of constraining the search to those nodes whose accumulated Euclidean distances are within a certain radius from the received signal, the search is performed in an unconstrained fashion. The tree search is defined instead by a tree configuration vector $n = [n_1, \dots, n_{MT}]$, which determines the number of child nodes (n_i) to be considered at each level. Therefore, the tree is traversed level by level regardless of the sphere constraints. Once the bottom of the tree is reached, the detector retrieves a list of N_{cand} candidate symbol vectors. It is worth noting that the set G composed of the N_{cand} selected symbol vectors may not correspond to the vectors of the set L with the smallest metrics given by the LSD, but provides sufficiently small metrics and diversity of bit values to obtain accurate soft information. A representation of an LFSD tree search is depicted in Figure 2 for a QPSK modulation and a tree configuration vector of $n = [1, 1, 2, 4]$.

3.1. Ordering algorithm

The performance of the LFSD soft-detector in un coded scenarios is strongly dependent on the ordering algorithm of the channel matrix and the choice of the tree configuration vector [7]. However, in the specific case of space-frequency-coded systems the effect of the ordering algorithm on the overall performance relies on the symbol power distribution in spatial and frequency directions. The structure of the Golden code generates a difference in the norms of the equivalent sub channels of each symbol in a pair, which allows for the implementation of an ordering procedure in order to improve the overall system’s performance.

An important feature when considering the optimum ordering approach is the tree configuration vector that will shape the search tree. As opposed to the LFSD detector presented in [7], the tree configuration vector for the detection of the Golden Code has been set to $n=[k,k,p,p]$, where $k < p$,

$p \leq P$ and $k < p$. With such a tree structure, if $p = P$ an exact ML search is performed in the first two levels of the tree, and therefore, there is no error propagation down to the next levels. Consequently, by ordering the equivalent channel matrix in such a way that the worst sub channel and the sub channel associated to the same pair are processed in the first two levels of the tree, respectively, the probability of finding vectors with smaller metrics is increased. The



proposed matrix ordering process only requires the computation of MT vector norms as opposed to other ordering algorithms such as the FSD [7] or the V-BLAST [8], which need to perform MT - 1 matrix inversion operations.

Considering the generation of bit LLRs for the proposed list fixed-complexity detector, comply with the equivalent system using the set G of the LFSF:

$$L_E(b_k|Y) \approx \frac{1}{2} \min_{b \in \mathcal{B}_{k,+1}} \frac{1}{\sigma^2} \|y - H_{eq} s\|^2 + b_{[k]}^T L_{A,[k]} - \frac{1}{2} \min_{b \in \mathcal{B}_{k,-1}} \frac{1}{\sigma^2} \|y - H_{eq} s\|^2 + b_{[k]}^T L_{A,[k]},$$

where for the sake of simplicity, the metric has been written as $\|y - H_{eq} s\|^2$ with $H_{eq} = \tilde{H} G$ as the effective equivalent channel.

IV. SIMULATION RESULTS

The performance of the overall system has been assessed by means of the bit error rate (BER) after the LDPC decoder. The bits of length of the LDPC block, code rate $R = 2/3$, 16-QAM modulation, OFDM symbol of 2048 carriers (2K) and 1/4 of guard interval. The simulations have been carried out over a Rayleigh channel (Typical Urban of six path, TU6), commonly used as the simulation environment for terrestrial digital television systems. Perfect CSI and non-iterative detection has been considered at the receiver.

4.1. Candidate choice

As has been previously stated, the calculation of the extrinsic information LE can be approximated using a list L or G with N_{cand} symbol vectors, respectively. When working with the ML metrics, i.e. the list L, the higher the number of candidates is, the more accurate the LE approximation is. Nevertheless, when considering the G list, the optimum value for N_{cand} will depend on the tree configuration vector \mathbf{n} . Thus, the higher the value of n_T , the better the approximation is. In order to choose a suitable number of candidates for the detection algorithm, a battery of tests have been carried out. Fig. 3 depicts the bit error performance after the detection stage for a given SNR of 14.4 dB and several values of N_{cand} and tree search configurations. The analyzed tree search configuration vectors \mathbf{n} have been obtained by setting $k = 1, 2, 3$ and $p = P$, which is equivalent to calculating $n_T = P^2, 4P^2, 9P^2$ Euclidean distances, respectively. On one hand, one can observe that the list ML approximation (8) might be considered accurate enough for $N_{cand} > 30$. On the other hand, a similar behavior for the fixed-complexity detector can be noticed, where the higher the value of k , the better the performance we obtain. Furthermore, it is noticeable that the ordering algorithm provides a performance enhancement such that the $k = 2$ LFSF approximates the BER values of the exhaustive ML detector.

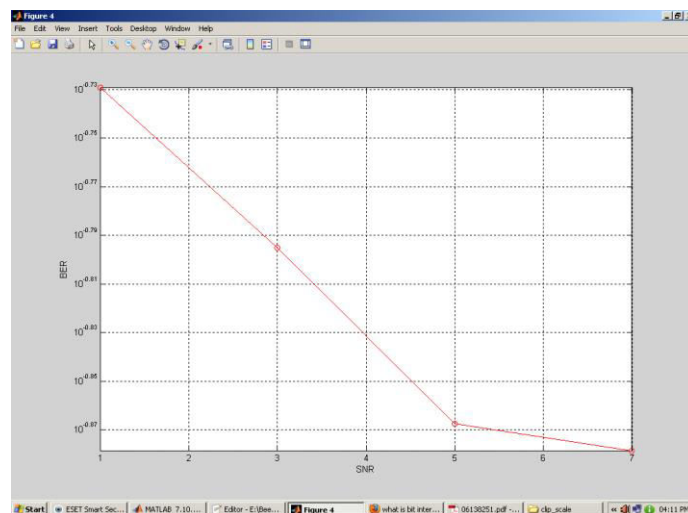


Figure 3 .BER performance of the LDPC-based SFBC OFDM transmission and reception scheme based on DVB-T2.



4.2. Performance comparison over DVB-T2 BICM system

This section presents the performance assessment and the complexity analysis of the new list fixed-complexity soft detector of the Golden code over a SFBC DVB-T2 broadcasting scenario. Fig. 4 shows the BER curves versus SNR for different configurations of the proposed algorithm. It is noteworthy that the ordering algorithm provides a gain of 0.4 compared to the non-ordering case for $nT = P2$ in the case $k = 1, p = P$ and $N_{cand} = 50$. In addition, the performance difference between LFSD and ordered LSD is 0.3 dB for the LFSD configuration $k = 1, p = P$ and $N_{cand} = 25$. However, this grows up to 1.3 dB with a less complex configuration, i.e. $k = 2, p = 8$. On the other hand, one should note that the LSD performance difference between $N_{cand} = 25$ and 50 is negligible resulting advantageous in the complexity degree of the algorithm.

In order to analyze the complexity of the detection algorithms, the cumulative distribution functions of the overall visited nodes have been depicted in Fig. 5. We see that the reduction of N_{cand} decreases the complexity of the LSD decoder compared to the LFSD. For $N_{cand} = 50$, 75 % of the LSD solutions are obtained visiting lower number of nodes than the LFSD algorithm. If N_{cand} is reduced up to 25, this value rises to 95 %. Despite these differences, the sequential nature of the LSD tree search and its variable complexity results in a problem for real hardware implementations. Nevertheless, the design of LFSD makes it possible a parallel architecture of the algorithm that can be fully pipelined and maintains fixed the search complexity.

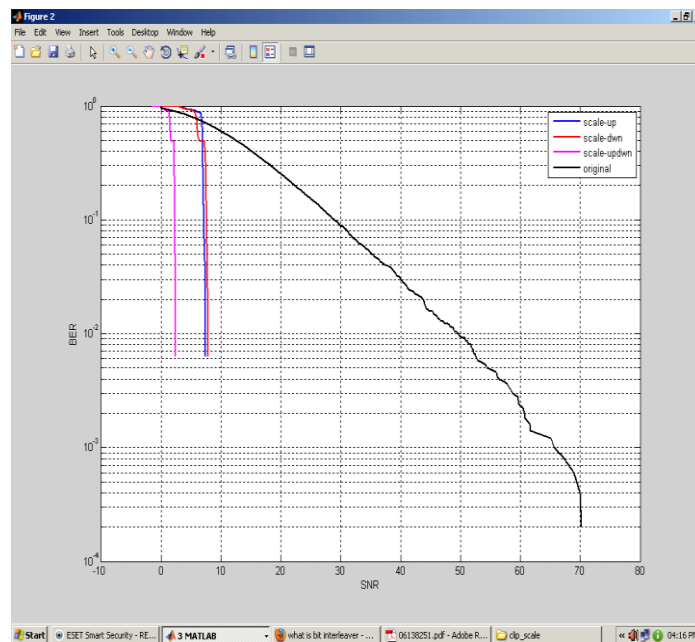


Figure3. BER performance of PAPR Reduction Based on Clipping and Differential Scaling

V. CONCLUSION

In this paper, we have presented a fixed-complexity detector for Golden codes and the analysis of its implementation on future digital TV broadcasting systems based on LDPC-coded BICM-OFDM. The main drawback of the LSD detection is its variable complexity that is strongly dependent on the noise and channel conditions, which leads to a complexity order upper-bounded by $O(P^4)$. A list fixed-complexity detector with a novel ordering algorithm is proposed in this paper with the aim of approaching the performance of the LSD using fixed complexity. The analysis of the number of candidates shows that the list approximation does not need a high list size in order to converge to the exact soft information value. Provided simulation results show that a close-to-optimal detection can be achieved considering a reduced number of candidates.

BER simulation results show the close-to-optimal performance of the proposed low-complexity detector in a typical LDPC-based DVB-T2 broadcasting scenario. The proposed detection algorithm can enable the realistic implementation and the inclusion of Golden codes in the forthcoming digital video broadcasting standards or in any similar BICM-OFDM system.



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